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Abstract. A focusing solution for bistatic forward-looking synthetic aperture radar (BFSAR) is presented. Forward-looking imaging is highly desirable in some potential applications, such as self-landing in bad weather, military surveillance, and navigation. Unfortunately, monostatic synthetic aperture radar reaches its limit when it is used in a forward-looking configuration. BFSAR can provide a high-resolution image in the forward-looking direction. However, due to the special forward-looking geometry, many proposed methods of deriving a bistatic point target reference spectrum (BPTRS) cannot handle the BFSAR data well. A modified Loffeld's bistatic formula (MLBF) for a forward-looking configuration is proposed first; it can get an accurate BPTRS of BFSAR. Then, a chirp scaling algorithm (CSA) based on MLBF is derived. CSA without interpolation allows high performance. Numerical simulations show that the proposed focusing solution can handle the BFSAR data well and achieve a high-resolution focused image. © The Authors. Published by SPIE under a Creative Commons Attribution 3.0 Unported License. Distribution or reproduction of this work in whole or in part requires full attribution of the original publication, including its DOI. [DOI: [10.1117/1.JRS.8.083586](https://doi.org/10.1117/1.JRS.8.083586)]

Keywords: bistatic forward-looking synthetic aperture radar; modified Loffeld's bistatic formula; chirp scaling algorithm.

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1 Introduction

Bistatic forward-looking synthetic aperture radar (BFSAR) has two platforms installed with a transmitter and receiver, respectively. Despite the separation of the two platforms, the BFSAR can still achieve a high azimuth resolution if a forward-looking geometry is used. Forward-looking imaging is highly desirable in some applications, but it has been a blind sector for monostatic synthetic aperture radar (SAR)^{1–3} for a long time. Therefore, BFSAR has recently received considerable attention.

The peculiarity and feasibility of BFSAR was studied in detail.^{4–6} Through the exploration of the limitation and potential of BFSAR, the best forward-looking geometry was proposed for achieving a high-resolution image. Moreover, some BFSAR experiments were carried out and the exciting imaging results were obtained.^{7–10} However, we can find that the imaging algorithms used in these experiments are mostly backprojection algorithms (time-domain algorithms). The time-domain algorithm can work well in arbitrary flight trajectories and no approximation is taken. However, it has a high computational cost and is not available for real-time imaging applications. Therefore, it is urgent to develop new frequency-domain imaging algorithms. Some theories of imaging algorithms for BFSAR have been reported. Based on the extended Loffeld's bistatic formula (ELBF) method,¹¹ a range-Doppler algorithm is developed.¹² But the ELBF method has its limitations in representing the bistatic point target reference spectrum (BPTRS). A chirp scaling algorithm (CSA) based on the method of Legendre polynomial

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extension was also proposed.¹³ The accuracy of this imaging solution is decided by the reserved order of an expending Taylor series. With the keystone transform method, a nonlinear chirp scaling algorithm for one-stationary BFSAR was derived.¹⁴ In addition, a modified Omega-k algorithm was also reported.¹⁵

To develop new frequency-domain imaging algorithms, we have to obtain the BPTRS of BFSAR first. The BPTRS derived by the method of series reversion (MSR)¹⁶ has a good focusing performance for the general bistatic configuration, even for extreme squint cases. Due to the series form, it is not easy for MSR to be used for imaging algorithm deduction, especially for chirp scaling and Omega-k algorithms.¹⁷ The Loffeld's bistatic formula (LBF) was first introduced in Ref. 18. In LBF, the contributions of the transmitter and receiver to the total Doppler frequency are assumed to be the same. This assumption results in the failure of LBF in the extreme configuration (i.e., spaceborne/airborne configuration). The ELBF¹¹ was proposed, but it cannot handle the large squint cases of bistatic SAR. The zeroth-order ELBF¹⁹ obtained two gradient equations to solve the Doppler contributions. However, the method would lead to some degradation when it is used in cases with extreme squint or with forward-looking cases to some extent.¹⁷

In this paper, a modified Loffeld's bistatic formula (MLBF) has been proposed. Compared to LBF¹⁸ and ELBF,¹¹ it can precisely represent the bistatic point target reference spectrum of bistatic forward-looking SAR. Then, a CSA based on BPTRS was derived. Because CSA is free of interpolation, this algorithm has an obvious superiority in efficiency. Finally, numerical simulations were carried out to validate the focusing solution for BFSAR.

2 Modified Loffeld's Bistatic Formula

The geometry configuration of BFSAR is shown in Fig. 1. The transmitter works in the side-looking mode and the receiver works in the forward-looking mode, respectively. The two platforms move along the y axis. The mathematical symbols and their definitions used in Fig. 1 are given as follows:

- t and τ : Time variables of range and azimuth.
- τ_{OT} and τ_{OR} : Zero Doppler times of the transmitter and receiver.
- r_{OT} and r_{OR} : The closest ranges from transmitter and receiver to the point target P.
- $R_T(\tau)$ and $R_R(\tau)$: Instantaneous slant ranges from the transmitter and receiver to the point target P.
- θ_{Tc} and θ_{Rc} : The squint angle of the transmitter and the forward-looking angle of the receiver at the composite beam center crossing time.
- v_T and v_R : Velocities of the transmitter and receiver, respectively.

Fig. 1 The geometry of bistatic forward-looking synthetic aperture radar (SAR).

The instantaneous slant ranges from the transmitter and receiver to the point target P at time τ are defined as

$$R_T(\tau) = \sqrt{r_{OT}^2 + (\tau - \tau_{OT})^2 v_T^2}, \quad (1)$$

$$R_R(\tau) = \sqrt{r_{OR}^2 + (\tau - \tau_{OR})^2 v_R^2}. \quad (2)$$

Hence, the echo data from target P after demodulation are

$$g(t, \tau) = \sigma_p w_r \left[t - \frac{R_T(\tau) + R_R(\tau)}{c} \right] w_a(\tau - \tau_c) \exp \left\{ j\pi k_r \left[t - \frac{R_T(\tau) + R_R(\tau)}{c} \right]^2 \right\} \cdot \exp \left[-j2\pi \frac{R_T(\tau) + R_R(\tau)}{\lambda} \right], \quad (3)$$

where $w_r(\cdot)$ and $w_a(\cdot)$ are window functions for range and azimuth, respectively; σ_p is the back-scattering coefficient of the point target P; τ_c is the central azimuth time of the composite azimuth antenna pattern; c is the velocity of light; f_0 and λ are the carrier frequency and wavelength; and k_r is the frequency modulated rate of linear frequency modulation signal.

Taking a two-dimensional FFT for Eq. (3), we get

$$g(f, f_\tau) = \sigma_p w_r(f) \exp \left\{ -j\pi \frac{f^2}{k_r} \right\} \int w_a(\tau - \tau_c) \exp[-j\phi_b(f, \tau)] d\tau, \quad (4)$$

where f and f_τ represent the range and azimuth frequency variables; the bistatic phase $\phi_b(f, \tau)$ is given as follows:

$$\begin{aligned} \phi_b(f, \tau) &= 2\pi(f + f_0) \frac{R_T(\tau) + R_R(\tau)}{c} + 2\pi f_\tau \tau \\ &= \frac{2\pi(f + f_0)}{c} \left[\sqrt{r_{OT}^2 + (\tau - \tau_{OT})^2 v_T^2} + \sqrt{r_{OR}^2 + (\tau - \tau_{OR})^2 v_R^2} \right] + 2\pi f_\tau \tau. \end{aligned} \quad (5)$$

From Eqs. (4) and (5), we can see that the bistatic phase term $\phi_b(f, \tau)$ contains a double square root and is included in the integral. It is difficult to obtain the BPTRS from Eq. (4) by directly applying the stationary phase.^{20,21} Thus, we split the bistatic phase term, Eq. (5), into two components as follows:

$$\phi_b(f, \tau) = \phi_T(f, \tau) + \phi_R(f, \tau), \quad (6)$$

$$\phi_T(f, \tau) = 2\pi \left[\frac{(f + f_0)}{c} R_T(\tau) + f_{\tau T} \tau \right], \quad (7)$$

$$\phi_R(f, \tau) = 2\pi \left[\frac{(f + f_0)}{c} R_R(\tau) + f_{\tau R} \tau \right], \quad (8)$$

where $\phi_T(f, \tau)$ and $\phi_R(f, \tau)$ are the phase terms contributed by the transmitter and receiver, respectively. $f_{\tau T}$ and $f_{\tau R}$ represent the instantaneous azimuth frequencies for the transmitter and receiver, respectively. In the LBF method,¹⁸ it is assumed that the contributions of the transmitter and receiver to the azimuth modulation are the same. The assumptions are shown as follows:

$$f_{\tau T} = f_{\tau R} = \frac{f_\tau}{2}. \quad (9)$$

However, the real azimuth modulations of the transmitter and receiver are not equal at all when the LBF is used in the extreme configuration (i.e., spaceborne/airborne configuration). Then, ELBF¹¹ formulates $f_{\tau T}$ and $f_{\tau R}$ as follows:

$$f_{\tau T} = k_T f_\tau, \quad (10)$$

$$f_{\tau R} = k_R f_\tau, \quad (11)$$

where k_T and k_R are the weighting factors, which are defined as the ratio of the time-bandwidth product (TBP) of transmitter and receiver to the total TBP. However, the ELBF shows a limitation in the high squint cases of bistatic SAR since the effect of squint angles on the instantaneous Doppler frequency is neglected.

The zeroth-order ELBF method¹⁹ makes the result of Eq. (12) as small as possible.

$$\|E\|^2 = (\tau - \tau_T)^2 + (\tau - \tau_R)^2, \quad (12)$$

where τ_T and τ_R are the transmitting and receiving points of stationary phases (PSPs). The variables $f_{\tau T}$ and $f_{\tau R}$ are included in τ_T and τ_R , respectively. This equation does not have an analytical solution, and an approximate solution can be found by using the least square method. The main idea of zeroth-order ELBF is to approximate the difference between the transmitting and receiving PSPs to zero. However, in this method, only the contributions of zeroth-order Doppler frequencies are considered. This would lead to some degradation when the method is used in forward-looking cases with large forward-looking angles.

In this paper, we try to solve the instantaneous azimuth frequencies $f_{\tau T}$ and $f_{\tau R}$ directly. Here, we redraw the geometries of the flight tracks of the transmitter and receiver, as shown in Fig. 2.

In Fig. 2, θ_T and θ_R are the instantaneous squint and forward-looking angles at time τ ; R_{Tc} and R_{Rc} are the slant ranges of the transmitter and receiver at the composite beam center crossing time τ_c . Suppose the transmitter and receiver both start flying at time τ_c ; after time $\Delta\tau$ we can get the following relationship:

$$\frac{R_{Tc} \sin \theta_{Tc} - R_{Tc} \cos \theta_{Tc} \tan \theta_T}{v_T} = \frac{R_{Rc} \sin \theta_{Rc} - R_{Rc} \cos \theta_{Rc} \tan \theta_R}{v_R}. \quad (13)$$

Meanwhile, the two instantaneous Doppler frequencies satisfy the following relationship:

$$f_\tau = \frac{f + f_0}{c} (v_T \sin \theta_T + v_R \sin \theta_R) = f_{\tau T} + f_{\tau R}. \quad (14)$$

Solving the equations composed by Eqs. (13) and (14), we can get the analytic expression of the frequencies $f_{\tau T}$ and $f_{\tau R}$. We expand $f_{\tau T}$ and $f_{\tau R}$ in their Taylor series as follows:

$$\begin{cases} f_{\tau T} = f_{\tau Tc} + A_{T1}(f_\tau - f_{\tau Tc}) + A_{T2}(f_\tau - f_{\tau Tc})^2 + A_{T3}(f_\tau - f_{\tau Tc})^3 \\ f_{\tau R} = f_{\tau Rc} + A_{R1}(f_\tau - f_{\tau Rc}) + A_{R2}(f_\tau - f_{\tau Rc})^2 + A_{R3}(f_\tau - f_{\tau Rc})^3 \end{cases}, \quad (15)$$

Fig. 2 The flight geometry of transmitter and receiver. (a) The geometry of transmitter's track. (b) The geometry of receiver's track.

where

$$\begin{cases} f_{\tau C} = f_{\tau TC} + f_{\tau RC} \\ f_{\tau TC} = (f_{\tau} + f_c)v_T \sin \theta_{Tc}/c \\ f_{\tau RC} = (f_{\tau} + f_c)v_R \sin \theta_{Rc}/c \end{cases} \quad (16)$$

Combined with Eqs. (13) and (14), coefficients $A_{T1} \dots A_{T3}$, $A_{R1} \dots A_{R3}$ can be obtained, then we get the analytic expressions of the frequencies $f_{\tau T}$ and $f_{\tau R}$. Although the results in Eq. (15) are more precise than those in Ref. 19 due to the high-order term in Eq. (15), the complexity of the method is greatly increased. It would make present difficulties when we derive the chirp scaling algorithm later. Therefore, some linear approximations are used here to solve Eqs. (13) and (14). We expand $\tan \theta_T$ and $\tan \theta_R$ in their Taylor series at $\sin \theta_T = \sin \theta_{Tc}$ and $\sin \theta_R = \sin \theta_{Rc}$, respectively, and only reserve the first-order term.

$$\begin{cases} \tan \theta_T = \tan \theta_{Tc} + \frac{\sin \theta_T - \sin \theta_{Tc}}{\cos^3 \theta_{Tc}} \\ \tan \theta_R = \tan \theta_{Rc} + \frac{\sin \theta_R - \sin \theta_{Rc}}{\cos^3 \theta_{Rc}} \end{cases} \quad (17)$$

Substituting Eq. (17) into Eq. (13) and combining Eq. (14), the equations are solved as follows:

$$\begin{cases} f_{\tau T}(f, f_{\tau}) = \frac{R_{Rc}v_T^2 \cos^2 \theta_{Tc} f_{\tau}}{R_{Tc}v_R^2 \cos^2 \theta_{Rc} + R_{Rc}v_T^2 \cos^2 \theta_{Tc}} \\ + \frac{v_T(f+f_0)(R_{Tc}v_R^2 \cos^2 \theta_{Rc} \sin \theta_{Tc} - R_{Rc}v_T v_R \cos^2 \theta_{Tc} \sin \theta_{Rc})}{c(R_{Tc}v_R^2 \cos^2 \theta_{Rc} + R_{Rc}v_T^2 \cos^2 \theta_{Tc})} \\ f_{\tau R}(f, f_{\tau}) = \frac{R_{Tc}v_R^2 \cos^2 \theta_{Rc} f_{\tau}}{R_{Tc}v_R^2 \cos^2 \theta_{Rc} + R_{Rc}v_T^2 \cos^2 \theta_{Tc}} \\ + \frac{v_R(f+f_0)(R_{Rc}v_T^2 \cos^2 \theta_{Tc} \sin \theta_{Rc} - R_{Tc}v_T v_R \cos^2 \theta_{Rc} \sin \theta_{Tc})}{c(R_{Tc}v_R^2 \cos^2 \theta_{Rc} + R_{Rc}v_T^2 \cos^2 \theta_{Tc})} \end{cases} \quad (18)$$

Although linear approximation is used, the max error made by this approximation (with Table 1 simulation parameters, which is discussed later in this paper, the forward-looking angle of the receiver is 45 deg) is 1.85×10^{-3} rad. Therefore, the error can be ignored and Eq. (18) can precisely present the contributions of the transmitter and receiver to the total azimuth modulation. After obtaining the instantaneous azimuth frequency of the transmitter and receiver, we expand Eqs. (7) and (8) at their points of the stationary phase τ_T and τ_R . The expanded series are truncated at the second-order term, given as

$$\phi_T(\tau) \approx \phi_T(\tau_T) + \frac{1}{2} \phi_T''(\tau_T)(\tau - \tau_T)^2, \quad (19)$$

$$\phi_R(\tau) \approx \phi_R(\tau_R) + \frac{1}{2} \phi_R''(\tau_R)(\tau - \tau_R)^2, \quad (20)$$

Table 1 System parameters in parallel tracks.

Parameters	Transmitter	Receiver
Carrier frequency	9.65 GHz	
Range bandwidth	100 MHz	
Velocity	200 m/s	
Pulse recurrence frequency sampling rate	600 Hz 180 MHz	
Position	(0,4,8) km	(10,0,4) km
Squint angle	0 deg	/
Forward-looking angle	/	45 deg

where

$$\tau_T = \tau_{OT} - \frac{cr_{OT}f_{\tau T}}{v_T^2 F_T}, \quad \tau_R = \tau_{OR} - \frac{cr_{OR}f_{\tau R}}{v_R^2 F_R}, \quad (21)$$

$$F_T = \sqrt{(f + f_0)^2 - \left(\frac{cf_{\tau T}}{v_T}\right)^2}, \quad F_R = \sqrt{(f + f_0)^2 - \left(\frac{cf_{\tau R}}{v_R}\right)^2}, \quad (22)$$

$$\phi_T''(\tau_T) = \frac{2\pi}{c} \frac{v_T^2 F_T^3}{r_{OT}(f + f_0)^2}, \quad \phi_R''(\tau_R) = \frac{2\pi}{c} \frac{v_R^2 F_R^3}{r_{OR}(f + f_0)^2}. \quad (23)$$

Substituting Eqs. (6), (19), and (20) into Eq. (4), we get

$$g(f, f_\tau) = \sigma_p w_r(f) \exp\left\{-j\pi \frac{f^2}{k_r}\right\} \exp\{-j[\phi_T(f, \tau_T) + \phi_R(f, \tau_R)]\} \\ \cdot \int w_a(\tau - \tau_c) \exp\left\{-\frac{j}{2}[\phi_T''(f, \tau_T)(\tau - \tau_T) + \phi_R''(f, \tau_R)(\tau - \tau_R)]\right\} d\tau. \quad (24)$$

Applying stationary phase techniques to the last exponent in Eq. (24), we get the bistatic stationary phase τ_b .

$$\tau_b = \frac{r_{OT}v_R^2 F_R^3 \tau_{OR} + r_{OR}v_T^2 F_T^3 \tau_{OT}}{v_T^2 F_T^3 r_{OR} + v_R^2 F_R^3 r_{OT}} - \frac{cr_{OT}r_{OR}(F_T^2 f_{\tau T} + F_R^2 f_{\tau R})}{v_T^2 F_T^3 r_{OR} + v_R^2 F_R^3 r_{OT}}. \quad (25)$$

Finally, we get the BPTRS of the BFSAR.

$$g(f, f_\tau) = \sigma_p \exp\left\{-j\pi \frac{f^2}{k_r}\right\} \exp\{-j\psi_{QM}\} \exp\left\{-\frac{j}{2}\psi_{BD}\right\}, \quad (26)$$

where

$$\psi_{QM} = \phi_T(f, \tau_T) + \phi_R(f, \tau_R) = 2\pi(f_{\tau T}\tau_{OT} + f_{\tau R}\tau_{OR}) + \frac{2\pi}{c}(r_{OT}F_T + r_{OR}F_R), \quad (27)$$

$$\psi_{BD} = \phi_T''(f, \tau_T)(\tau_b - \tau_T)^2 + \phi_R''(f, \tau_R)(\tau_b - \tau_R)^2 \\ = \frac{2\pi v_T^2 v_R^2 F_T^3 F_R^3}{c(f + f_0)^2(v_T^2 F_T^3 r_{OR} + v_R^2 F_R^3 r_{OT})} \\ \cdot \left[(\tau_{OT} - \tau_{OR}) - \frac{c}{v_T^2 v_R^2 F_T F_R} (r_{OT}v_R^2 F_R f_{\tau T} - r_{OR}v_T^2 F_T f_{\tau R}) \right]^2. \quad (28)$$

ψ_{QM} can be considered as the quasi-monostatic phase term, and ψ_{BD} is defined as the bistatic deformation phase term. Before implementing an imaging algorithm, the bistatic deformation phase term should be compensated. The method proposed above can be considered as an MLBF.

3 CSA for the Bistatic Forward-Looking SAR Processing

Instead of interpolation, chirp phase multiplication is used in CSA to correct the range cell migration (RCM). It is an efficient algorithm. However, due to the unknown scaling factor, it is complex to derive CSA based on the BPTRS obtained by the MLBF.

After compensating the bistatic deformation phase term, we transform Eq. (26) into a range-Doppler domain and obtain the expression as

$$g(t, f_\tau) = \sigma_p \exp \left[-j \frac{2\pi}{c} (r_{OT} D_T + r_{OR} D_R) f_0 \right] \exp[-j2\pi(B \cdot \tau_{OT} + E \cdot \tau_{OR})f_0] \\ \cdot \exp[-j2\pi(A \cdot \tau_{OT} + D \cdot \tau_{OR})f_\tau] \exp \left\{ j\pi k_m \left[t - \frac{R(f_\tau)}{c} \right]^2 \right\}, \quad (29)$$

where

$$A = \frac{R_{Rc} v_T^2 \cos^2 \theta_{Tc}}{R_{Tc} v_R^2 \cos^2 \theta_{Rc} + R_{Rc} v_T^2 \cos^2 \theta_{Tc}}, \quad (30)$$

$$B = \frac{v_T (R_{Tc} v_R^2 \cos^2 \theta_{Rc} \sin \theta_{Tc} - R_{Rc} v_T v_R \cos^2 \theta_{Tc} \sin \theta_{Rc})}{c (R_{Tc} v_R^2 \cos^2 \theta_{Rc} + R_{Rc} v_T^2 \cos^2 \theta_{Tc})}, \quad (31)$$

$$D = \frac{R_{Tc} v_R^2 \cos^2 \theta_{Rc}}{R_{Tc} v_R^2 \cos^2 \theta_{Rc} + R_{Rc} v_T^2 \cos^2 \theta_{Tc}}, \quad (32)$$

$$E = \frac{v_R (R_{Rc} v_T^2 \cos^2 \theta_{Tc} \sin \theta_{Rc} - R_{Tc} v_T v_R \cos^2 \theta_{Rc} \sin \theta_{Tc})}{c (R_{Tc} v_R^2 \cos^2 \theta_{Rc} + R_{Rc} v_T^2 \cos^2 \theta_{Tc})}, \quad (33)$$

$$\mu_{T1} = A \cdot \frac{c f_\tau}{f_0 v_T} + B \cdot \frac{c}{v_T} \quad \mu_{T2} = B \cdot \frac{c}{v_T}, \quad (34)$$

$$\mu_{R1} = D \cdot \frac{c f_\tau}{f_0 v_R} + E \cdot \frac{c}{v_R} \quad \mu_{R2} = E \cdot \frac{c}{v_R}, \quad (35)$$

$$D_T = \sqrt{1 - \mu_{T1}^2} \quad D_R = \sqrt{1 - \mu_{R1}^2}. \quad (36)$$

In Eq. (29), the frequency-modulated rate k_r in range is changed by the coupling of the range and azimuth, and the new chirp rate k_m in range-Doppler domain is given as

$$k_m = \frac{k_r}{1 - \frac{c k_r f_\tau^2}{f_0^2} \left(\frac{A^2 r_{OT}}{D_T^3 v_T^2} + \frac{D^2 r_{OR}}{D_R^3 v_R^2} \right)}. \quad (37)$$

In Eq. (29), $R(f_\tau)$ is the range migration of a target and is defined as

$$R(f_\tau) = c \cdot (B \cdot \tau_{OT} + E \cdot \tau_{OR}) + \frac{(1 - \mu_{T1} \mu_{T2}) r_{OT}}{D_T} + \frac{(1 - \mu_{R1} \mu_{R2}) r_{OR}}{D_R}. \quad (38)$$

We assume the range chirp scaling function for the BFSAR as follows:

$$H_{CS} = \exp \left\{ j\pi k_m C_s \left[t - \frac{R_{\text{ref}}(f_\tau)}{c} \right]^2 \right\}, \quad (39)$$

where C_s is the unknown scaling factor. $R_{\text{ref}}(f_\tau)$ is the range migration of the reference target, given as

$$R_{\text{ref}}(f_\tau) = c \cdot (B \cdot \tau_{OT} + E \cdot \tau_{OR}) + \frac{(1 - \mu_{T1} \mu_{T2}) r_{OT_ref}}{D_T} + \frac{(1 - \mu_{R1} \mu_{R2}) r_{OR_ref}}{D_R}. \quad (40)$$

In Ref (41), r_{OT_ref} and r_{OR_ref} are the closest ranges from the transmitter and receiver to the reference target. (The target located at the middle of the imaging scene is usually chosen as the reference target.) We multiply Eq. (29) by Eq. (39) and implement FFT in the range direction, and then get

$$G_1(f, f_\tau) = \sigma_p \exp \left[-j \frac{2\pi}{c} (r_{OT} D_T + r_{OR} D_R) f_0 \right] \exp[-j2\pi(B \cdot \tau_{OT} + E \cdot \tau_{OR}) f_0] \\ \cdot \exp[-j2\pi(A \cdot \tau_{OT} + D \cdot \tau_{OR}) f_\tau] \exp \left[-j\pi \frac{f^2}{(1 + C_s) k_m} \right] \\ \cdot \exp \left[-j2\pi f \frac{R(f_\tau) + C_s R_{\text{ref}}(f_\tau)}{(1 + C_s) c} \right] \exp \left\{ j\pi k_m \frac{C_s [R(f_\tau) - R_{\text{ref}}(f_\tau)]^2}{(1 + C_s) c^2} \right\}. \quad (41)$$

In Eq. (41), we can clearly see that the total RCM is

$$\text{RCM} = \frac{R(f_\tau) + C_s R_{\text{ref}}(f_\tau)}{1 + C_s}. \quad (42)$$

Because the translational invariant case is used in this paper, we make some linear approximations.¹² The approximations are given as

$$\tau_{OT} = p_0 + \tau_{OR}, \quad (43)$$

$$r_{OT} = p_1 + p_2 r_{OR}, \quad (44)$$

where p_0 , p_1 , and p_2 are all coefficient factors. Therefore, we can transform the total RCM as follows:

$$\text{RCM} = c[B \cdot p_0 + (B + E)\tau_{OR}] + \frac{(1 - \mu_{T1}\mu_{T2})p_1}{D_T} + \frac{C_s r_{OR, \text{ref}}}{1 + C_s} \left[\frac{(1 - \mu_{T1}\mu_{T2})p_2}{D_T} + \frac{1 - \mu_{R1}\mu_{R2}}{D_R} \right] \\ + \frac{r_{OR}}{1 + C_s} \left[\frac{(1 - \mu_{T1}\mu_{T2})p_2}{D_T} + \frac{1 - \mu_{R1}\mu_{R2}}{D_R} \right], \quad (45)$$

where the last term of the RCM is a range variant term. In order to remove the range variant of the total RCM on the Doppler frequency, we let

$$\frac{r_{OR}}{1 + C_s} \left[\frac{(1 - \mu_{T1}\mu_{T2})p_2}{D_T} + \frac{1 - \mu_{R1}\mu_{R2}}{D_R} \right] = (1 + p_2)r_{OR}. \quad (46)$$

Then, the analytic formula of the scaling factor C_s is obtained as

$$C_s = \frac{1}{1 + p_2} \left[\frac{(1 - \mu_{T1}\mu_{T2})p_2}{D_T} + \frac{1 - \mu_{R1}\mu_{R2}}{D_R} \right] - 1. \quad (47)$$

Therefore, after substituting Eq. (47) into Eq. (41), we can rewrite Eq. (41) without unknown variables. Then, we use the following matching filters to complete the image focusing:

Fig. 3 Block diagram of chirp scaling algorithm (CSA) used in bistatic forward-looking SAR.

$$H_{RC} = \exp \left[j\pi \frac{f^2}{(1 + C_s)k_m} \right] \cdot \exp \left\{ j \frac{2\pi C_s r_{OR_ref}}{c(1 + C_s)} \left[\frac{(1 - \mu_{T1}\mu_{T2})p_2}{D_T} + \frac{1 - \mu_{R1}\mu_{R2}}{D_R} \right] f \right\}, \quad (48)$$

$$H_{RES} = \exp \left\{ -j\pi k_m \frac{C_s [R(f_\tau) - R_{ref}(f_\tau)]^2}{(1 + C_s)c^2} \right\}, \quad (49)$$

$$H_{AC} = \exp[j2\pi(A \cdot \tau_{OT} + D \cdot \tau_{OR})f_\tau] \exp \left[j \frac{2\pi}{c} (r_{OT}D_T + r_{OR}D_R)f_0 \right] \cdot \exp[j2\pi(B \cdot \tau_{OT} + E \cdot \tau_{OR})f_0], \quad (50)$$

Fig. 4 Focusing results. (a) Processing result using Loffeld's bistatic formula (LBF). (b) Processing result using extended LBF. (c) Processing result using modified LBF (MLBF). (d) Processing result using method of series reversion. (e) Comparison results of the azimuth profiles obtained from Figs. 4(c) and 4(d).

where H_{RC} is used for range compression (RC), the second range compression, and the bulk range cell migration correction; H_{AC} is used for azimuth compression; and H_{RES} is used to remove the residual phase term introduced by the chirp scaling multiplication. The corresponding block diagram of the CSA for the BFSAR is shown in Fig. 3.

4 Simulation Results

In order to verify the focusing solution for the BFSAR, two simulation experiments are carried out in this section. The first experiment is to determine whether the BPTRS obtained by the MLBF is appropriate for the BFSAR case and to simultaneously compare the performance of the MLBF with those of other proposed methods. The second experiment is to validate the effectiveness of the proposed CSA.

The simulation parameters are listed in Table 1. We use the analytical BPTRS to focus the BPTRS obtained by LBF,¹⁸ ELBF,¹¹ MLBF, and the spectra derived from the MSR using the fourth-order expansion.¹⁶ The focusing results are shown in Fig. 4.

From Figs. 4(a) and 4(b), we can see that the LBF and ELBF have severe degradation in the azimuth direction. They are not appropriate for bistatic forward-looking SAR cases. In general, the LBF method and ELBF method reach their limit when the forward-looking angle is 30 and 40 deg, respectively. Figures 4(c) and 4(d) reveal that MLBF and MSR are all focused on the point target. Furthermore, Fig. 4(e) shows the azimuth profiles of the MLBF and MSR. It is clear that the method proposed in this paper agrees with the MSR. However, the resulting accuracy of the spectrum from the MSR is dependent on the number of terms in the expansion. Here, we use the fourth-order expansion of the MSR. However, the spectrum of the MLBF is a closed form with a second term and still has a good performance. In addition, it is not easy for the MSR to be used for imaging algorithm deduction.

Fig. 5 CSA imaging results based on the bistatic point target reference spectrum obtained by MLBF. (a) The locations of simulated targets. (b) The contours of final imaging result with 30 dB dynamic range. (c) The azimuth profile of the target P9. (d) The range profile of the target P9.

Table 2 Image quality parameters.

Targets	Range			Azimuth		
	PSLR (dB)	ISLR (dB)	IRW (cells)	PSLR (dB)	ISLR (dB)	IRW (cells)
PT1	−12.96	−9.77	1.54	−14.42	−10.96	6.14
PT5	−13.02	−9.80	1.54	−14.53	−11.10	6.06
PT9	−12.96	−9.78	1.55	−14.52	−11.04	6.20

PSLR, peak sidelobe ratio; ISLR, integrated sidelobe ratio.

The CSA imaging results are shown in Fig. 5.

Figure 5(a) shows the locations of the simulated targets, where the distances between two adjacent targets along the range and azimuth directions are, respectively, 400 and 300 m. Figure 5(b) represents the contours of the final imaging result. The dynamic range shown in this picture is 30 dB. In order to further evaluate the imaging quality, Figs. 5(c) and 5(d) present the impulse profiles of the target P9 in the azimuth and range directions, respectively. The peak sidelobe ratio (PSLR) of the azimuth profile is −14.52 dB, and the integrated sidelobe ratio (ISLR) is −11.04 dB. The PSLR of the range profile is −12.96 dB, and the ISLR is −9.78 dB. More image quality parameters are listed in Table 2. The ideal impulse response width (IRWs) of the azimuth and range are 6.04 and 1.52 cells (or samples), respectively. We can find that all the targets are well focused.

5 Conclusions

A focusing solution for bistatic forward-looking SAR was presented in this paper. First, an MLBF was proposed to obtain the BPTRS. Then, a chirp scaling algorithm based on the BPTRS was derived. Compared to other imaging algorithms, CSA is free of interpolation. Finally, two simulation experiments were carried out to validate the focusing solution. The simulation results showed that the BPTRS obtained by the MLBF was more precise than the LBF and ELBF, and that the focusing capability of the derived CSA is high.

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